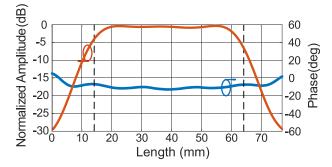
	Frequency	Size	Amplitude	Phase	Efficiency	Feeding
	(GHz)		Variation (dB)	Distortion (deg.)	(%)	Mechanism
[2]	11.5	$1.93\lambda$	$\pm 10$	$\pm 20$	50	Slotted Waveguide
[6]	76	$6.5\lambda$	$\pm 3$	$\pm 30$	50	Coupling Windows
[7]	9.35	$5.67\lambda$	-	-	81	Multiple Reflector System and Twin Pin Feeder with Leaky PRS
						$(\beta > \alpha)$
(this work)	15	$2.5\lambda$	$< \pm 1.5$	$<\pm5$	>90	Leaky SIW T-Junction and Single-input Microstrip Feed
						$(\beta pprox \alpha)$

#### TABLE 1. Feeding network performance comparison.

different from zero ( $H_y \neq 0$ ). On the other hand, inside the PPW, there are no components in the direction of propagation ( $E_y = 0, H_y \approx 0$ ) as expected for a TEM mode.

The normalized amplitude distribution and the phase are further depicted in Fig. 7, where it can be observed that the amplitude is uniform along most of the launcher aperture and starts to decay by about 5 dB when approaching the PEC sections at the end of the T-junction arms. On the other hand, the phase maintains small variations of  $5^{\circ}$  or less along the entire aperture while a maximum variation of about 1.5 dB is observed. It should also be mentioned that our aperture profile provides a more uniform distribution when compared to [13], since in that work phase and magnitude variations of more than 25° and 2 dB were observed, respectively. Some comparisons between the proposed structure and previous feeding networks for slot based planar antennas found in the literature has also been included in Table 1. This comparison shows the improvement with respect to previous alternatives to feed slot arrays in terms of compactness and efficient propagation.



**FIGURE 7.** The normalized amplitude (left) in dB and the phase (right) in a transverse plane within the end-to-end for the dominant component  $E_z$ . The two dashed black lines define the ends of the PRS wall.

Following these developments and modal characterization, an end-to-end test device using two launchers has been designed using the commercial full-wave simulation tool CST Microwave Studio [22]. See Fig. 8 where the simulated electric fields are depicted and show uniform propagation within the PPW region.

Depending on the desired feed system requirements, it is also possible to obtain a similar uniform field distribution but for a wider aperture by means of introducing some

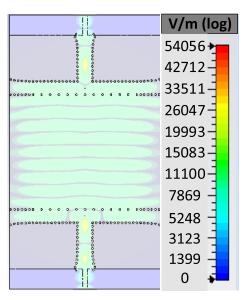
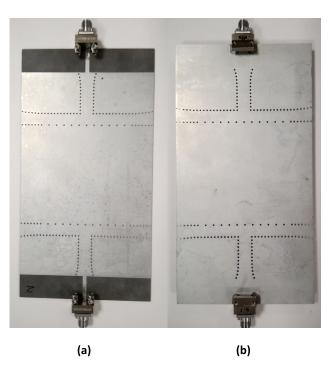


FIGURE 8. Simulated electric fields within the examined PCB test circuit using two launchers. A collimated or uniform TEM field profile can be observed inside the PPW region.

asymmetry in the feed. This can allow for the leakage rate to be tailored as desired without affecting the pointing angle as in [23]. Such a tapered LW distribution could allow for uniform feeding in larger arrays while maintaining the desired parallel-plate propagation at broadside. Future work can include the use of this tapered leakage when considering slot array feeding.

### **III. MEASUREMENT RESULTS AND DISCUSSION**

As a proof of concept, an end-to-end structure has been manufactured on a ROGERS RT5880 substrate with a thickness h of 0.79 mm and a rated relative permittivity  $\varepsilon_r = 2.2$  at 10 GHz. This substrate was selected due to its capability to support a unimodal propagation. A photograph of the realized prototype is reported in Fig. 9 while measurements are shown in Fig. 10. It should be mentioned that in real antenna applications for example, a second launcher would not be included. Therefore measurements and simulations are used to demonstrate that the power is actually launched into the PPW and is able to propagate without significant losses, confirming its capability to feed any element placed

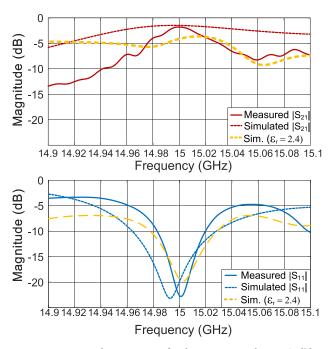


**FIGURE 9.** The manufactured prototype, top conducting layer on left (a) and bottom layer on the right (b), to work at 15 GHz on Rogers RT5880 with  $\varepsilon_r = 2.2$  (rated) for the relative dielectric constant.

within the PPW. The relevant parameters defined for this PPW launcher to achieve a design frequency of 15 GHz are as follows: W = 6.8 mm, W' = 10.2 mm,  $W_o = 2.35 \text{ mm}$ , P = 4.5 mm and d = 1 mm.

The two launchers were placed several wavelengths apart for practical demonstration purposes. This introduced some conductor and dielectric losses which slightly increased the port-to-port insertion losses, but still the launcher is operating as expected as shown in Fig. 10. The measured  $|S_{21}|$  for the test structure is about -1.3 dB at the design frequency of 15 GHz and  $|S_{11}| < -20$  dB. The electromagnetic coupling between the two launchers is not of concern because the complete end-to-end structure was simulated in CST [22] and no significant losses were found, as shown in Fig. 10 for  $\varepsilon_r = 2.2$ . This is important because the launchers are not in the respective far-field regions for each wave-guiding structure, which we consider to be  $32\lambda_g$  following  $R = 2D^2/\lambda_g$  [24] (where  $\lambda_g = \frac{1}{f\sqrt{\varepsilon_r \varepsilon_0 \mu_0}}$  and  $\varepsilon_0$  and  $\mu_0$  are the free-space permittivity and permeability, respectively, and D is the length of the leaky aperture). Also, the measurements are in good agreement with the simulations as well as the center frequency for the structure designed using LW theory and the developed TEN circuit model.

Higher losses for the measured structure at the design frequency can be explained by the importance of the substrate relative dielectric constant as well as the fabrication tolerances for via placement and via diameters. More specifically, the via drilling processes defines the exact via placement and its diameters and small variations from any nominal value can



**FIGURE 10.** Measured S-parameters for the structure under test (solid lines) compared to simulations (dashed lines) using the rated values for the dielectric  $e_r = 2.2$  at 10 GHz. The difference between the measurements and simulations can be attributed to the practical variation of the relative permittivity of the substrate (see yellow dashed lines). Regardless of these practicalities the launcher is still operating as expected, showing proof of concept.

result in minor performance variations and small frequency shifts away from the original design frequency. For example, in our simulation model we considered a  $\pm 5\%$  variation in the diameters of the all vias within the transition structure and about a 0.5% frequency shift in the minimum of  $|S_{11}|$ was observed (results not reported for brevity). Also, for any minor variation in  $\varepsilon_r$  (see Fig. 10) port matching can be maintained, however the maximum value for  $|S_{21}|$  can be shifted in frequency because the originally designed  $\alpha \approx \beta$  condition is no longer preserved, and, at the original frequency. This can be observed in Fig. 10 when considering a variation of the relative permittivity in the material of  $\varepsilon_r = 2.4$  since good port matching is still obtained at 15.0 GHz ( $|S_{11}| < -15.0$  dB) while  $|S_{21}|$  is less than -4.0 dB at about 15.02 GHz as observed for the simulations. Despite these practicalities, the measured performance is still in good agreement with the full-wave simulations.

The structure is inherently narrow band due to the  $\alpha \approx \beta$  condition at the design frequency. This can be observed in Fig. 10 for both the measurements and the simulations as  $|S_{11}| < -10$  dB from about 14.98 GHz to 15.02 GHz. Techniques exist to enhance the bandwidth of such LW apertures and can be applied to both radiating leaky-wave antennas and non-radiating structures as in this work. For example, in [25] a double-cavity leaky-wave antenna with an improved operational frequency range was made possible by two stacked PRS layers.

## **IV. CONCLUSIONS**

In this paper, design guidelines and measured results for a novel PPW TEM mode launcher for feeding planar circuits and low-cost antenna systems has been presented. This SIW to PPW transition is compact and maintains a low profile for simple fabrication and offers  $50-\Omega$  microstrip feeding. By proper design of the structure, uniform and bound propagation at broadside (with respect to the leaky SIW sidewall) can be achieved within the PPW region. Due to the practical substrate variations and SIW technology fabrication tolerances, the measurements of the demonstrator circuit are not exactly as per the full-wave simulations. However, measurements of this end-to-end test structure still suggest that the two launchers operate at about 15 GHz, as per design, and follow the developed LW theory and waveguide dispersion analysis.

It should also be mentioned that our proposed PPW TEM planar launcher can be re-designed when using different permittivity substrates and when considering operation at higher millimeter-wave frequencies. Also, the relatively narrow band behavior of the structure could be improved by employing a double layer of PRSs. This can create two cavities where the modes can couple as studied in [25] increasing the possible frequency range of the structure. Our proposed PPW launcher could lead to other kinds of SIW launchers, such as surface-wave launchers when considering  $TM_0$  surface-wave propagation on grounded dielectric slabs as briefly examined in [26] and for end-fire radiation, new planar antennas, or to other wave guiding structures and other new transition circuits.

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